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Analysis of Pruned DFT Spread Filter Bank Multicarrier System for Low PAPR

R. Sittalatchoumy, Malarvizhi Muthuramalingam

Department of ECE, College of Engineering (Anna University), Guindy, Chennai, India.

ABSTRACT

Despite being a potential waveform for automation for the fifth genesis, FBMC has notable shortcomings, including high PAPR and cost escalation. Therefore, to develop a waveform contender with high spectral efficiency with low complexity and less peak power ratio, a method has been proposed called Pruned DFT (discrete Fourier Transform) spread along with one tap scaling, we can reduce PAPR. The fashion suggested here has one and the consistent ratio of peak-average power as linearly precoder OFDMA nevertheless uses solo bit transmission per symbol and has much lower out-of-band emigrations. The use of prototype filters is also more stringent than traditional FBMC systems.

KEYWORDS

Fourier transform spread; Half input matrix; Hermite filters; Multicarrier filter banks; Orthogonal frequency division multiplexer; Pruned discrete.

1. INTRODUCTION

An analysis of the multicarrier system results in the creation of rapidly evolving technology that connects everyone from anywhere in the world. The technique with the addition of a prefix that uses a rectangular set of subcarriers i.e., OFDM is the widespread case predicted for reliable comparability. Even so, cyclic prefixes, a lack of frequency and time synchronization, and poor out-of-band emission encourage FBMC innovation.

A new multi-carrier waveform called the Filter Bank Multicarrier System uses a bank of filters to produce subcarriers with better spectral shapes. CP scarcity can be equalized by composing a proto filter by diminishing interference among subcarriers. Furthermore, the use of offset Quadrature Amplitude Modulation can be advantageous in maximizing transmission bandwidth [1]. It substitutes the less stringent real orthogonality criteria for the complex orthogonality constraint. The immersion in the unreal part leads to natural hindrance, causing channel evaluation and multiple input and Multiple-Output (MIMO) to become more grueling [2]. In addition to inherent interference, solitons like a DAC with a low aspiration or a nonlinear power amplifier represent an even bigger issue in real-world systems since they undermine the enhanced spectrum confinement of FBMC [3].

We suggest a unique modulation approach based on a trimmed DFT in conjunction with one delay weighing to get over all those issues. Thus, our suggested technique offers less PAPR while maintaining all the fundamental characteristics of normal FBMC, such as truncated OOB The necessary adjustments are achieved by using one-tap scaling instead of exchanging complex real components of pruned DFT to maintain power leakage, low delay, and good spectrum strength**.** Precoding a DFT matrix and spreading it with input [4]. Although there are many reducing methods such as clipping, and nonlinear companding, we apply DFT spread because all these methods require high computational complexity and side information.

The prototype filter is further condensed to a temporal duration of 1.5, where F stands for the subcarrier spacing. Instead of temporal modification, which uses a modified prototype filter, the frequency is spread out more [5]. Thus, it has a lower overhead than conventional FBMC. Finally, we compare our proposed method with the traditional OFDM method and infer their differences.

2. LITERATURE REVIEW

Numerous methods exist to lower the power ratio between peak and average power. In Partial transmission, data is fed into the transmitter divided into V blocks, and zeros are addedup to length and then given into IFFT. There are three methods of PTS implementation. They are adjoining, interlaced, and random [6]. After IFFT each output is amplified by a time delay factor for phase rotation {a} and finally, the value with optimum PAPR is transmitted to the channel. In FBMC OQAM with simple DFT spreading, FFT is used to pass input data symbols through, where real and imaginary corridors are separated and multiplied by phase factor and passed through IFFT. The prototype filter is applied after copying the IFFT output to an overlapping factor. Finally, the output is supplemented with the overlap sum. Since the real and imaginary parts are delayed by time shift called Offset Quadrature amplitude modulation [7].

We can also use a polyphase network filter to reduce complexity. Therefore, simple DFT overcomes the complicatedness problem but only has a borderline reduction in peak power. Different shift patterns have been optimized and multiplied with the IFFT affair in a constant shift in the multicarrier (ITSM) algorithm to shift the peak power and increase the PAPR rate [8].

But complexity also increases with an increase in shift patterns Tone reservation and DFT with single carrier phase shift effectled to high involution whereas General DFT spreading- reduces significantly further than DFT. In Section III, We give a brief summary of the OFDM system, followed by Section IV having note of FBMC is described with a transmission system model [9].

OOB emissions are also covered in Section, along with the concept of trimmed DFT spread FBMC and the operation of the proposed method's PAPR and Bit. We discuss Bit Error Ratio (BER) and PSD in Section VI, where we also offer simulations [10].

3. OUTLINE OF FBMC OQAM

Lack of PAPR and strong OOB emission are caused by spectral exposure of the sinc function and the ongoing inclusion of multiple carriers in OFDM, respectively. As a result, the Filter Bank Multicarrier System approach, which conveys a well-sectional subchannel in both the domain (i.e.) time and frequency solves the hindrance of the linearly precoded OFDMA. It also hinders equality because there is no cyclic prefix [11].

To maximize throughput for FBMC systems, quadrature amplitude modulation (OQAM) shifts real and imaginary signals by half the symbol time. As a result, spectrum segregation of signals occurs [12]. The maindistinction is the removal of OFDM in favor of a multicarrier system that utilizes filter banks, where the bank with synthesis filter (SFB) replaces the FFT plus CPout and the bank with analysis filter restores the IFFT plus CPin (AFB Figure 2 illustrates how the filter banks on both the sides of sender and collector are made up of a batch of N filters that transform signals of N put in into N outages. Synthesis filter bank respectively and analysis filter bank, are the terms used to project the filter banks in Figure 1.

The transmitter uses a synthesis filter bank to pass the input signal in parallel form. As a result of a parallel-to-serial converter, now vectors are in the serial form once more. The opposite of what happens on the sender side occurs on the collector. This is described by synthesis-analysis architecture shown in Figure 1 is used in MC communication systems and is known as transmulitplexer or TMUX [13].

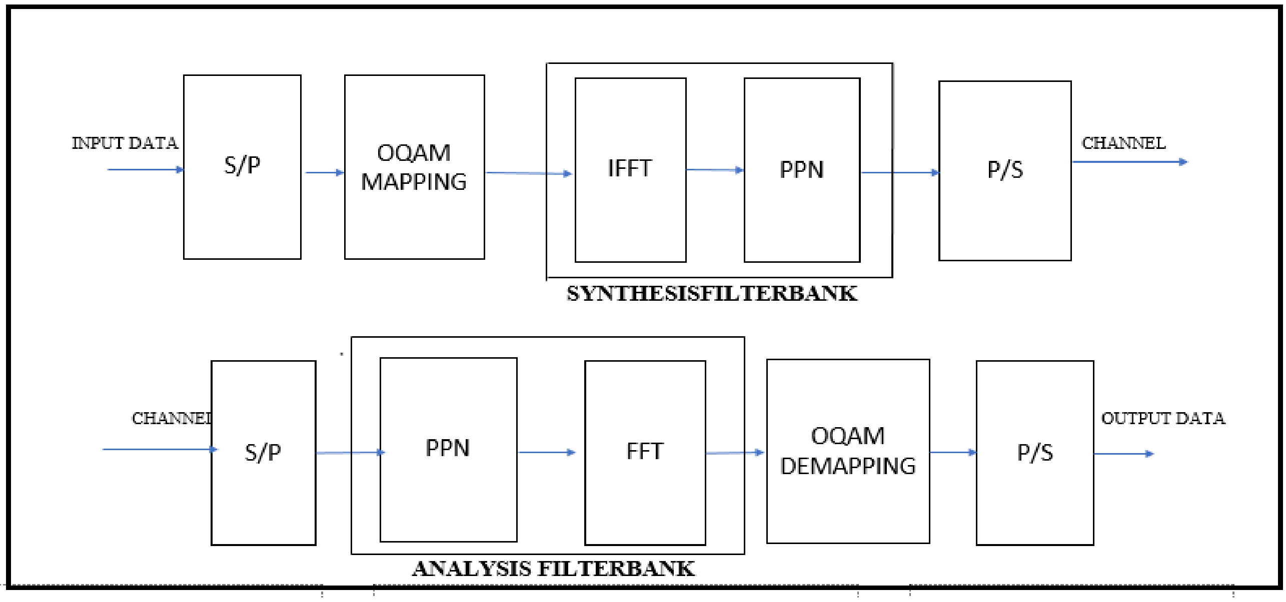

Fig. 1 Block Diagram of FBMC

3.1 System Architecture

The bank's collector and sender, early processing, and processing of OQAM are the four primary processing units of TMUX.

3.1.1 Early and Late Processing of OQAM

The working of OQAM is determined by two stages. The initial process is to convert the imaginary to real, which separates the real and imaginary parts of symbols into two distinct symbols. This process is referred to as lurching [14]. It yields a two-fold increase in the sampling rate. Sequence multiplication is the second operation. After OQAM processing, the signals to the IFFT are solely unreal or fictitious [15].

There are additionally two operations in post-processing. 1)Sequential multiplication and 2) Conversion from real to complex. Phase staggering techniques cause the fictitious symbol to lag the actual value, whereas QAM modulation does not. and the term "offset" refers to the temporal difference between the real and imaginary halves of a complex symbol that is the same as half of the subchannel spacing inverse [16].

3.1.2 Synthesis and Analysis Filter Bank

At the transmitter side, a Synthesis filter is utilized. It is made up of as many samplers and synthesis filters as there aresubcarriers [17]. The input signals are initially sampled using half of the M, and after that, a bank of prototype filters is used to filter them. On the other hand, a bank of analysis filters and accompanying down samplers make up the receiver. The output signal is created by down sampling the input signal by a factor of M /2 after the analysis filter has first filtered the input signal [18].

3.1.3. Prototype Filter Design

The prototype filter refers to the carrier with no phase shift from which the subsequent filter members are produced through a shifting phase in a linear fashion. The filter coefficients are amplified by e j2k/M, which causes the frequency response to shifting by k / M. When all of the FFT outputs are taken into account, a bank of M filters is produced, with 1/M, as the unit on the frequency axis. The simplest clear out frequency response is non-zero by way of the Nyquist pulse shaping foundation at frequencies that are integer multiples inverse of M indicating the orthogonality criterion [19]. The representation filter in the frequency domain is shown below: D0=1; D1=0.971960; D2=0.707; D3=0.235147.
By employing this prototype filter, FBMC offers good side lobe attenuation, increasing spectral efficiency and satisfying the equation below.

$$\frac{1}{K}\sum_{k=-k+1}^{K} |D_k| \frac{1}{K} \quad (1)$$

By using the IFFT on the frequency responses, the initial prototype filter's impulse response is provided as D[m].

$$d[m] = 1 + 2\sum_{k=1}^{K-1} D_k cos\,[\frac{2\pi k}{MK} m] \quad (2)$$

4. PROPOSED SYSTEM

A novel scaling-down method named pruned DFT spread with one tap scaling is proposed. The advantages of this method include low latency, restoring real and complex orthogonality, reducing OOB emission due to Hermite filtering, minimal entanglement due to on-tap equalization, robustness for doubly selective channels, and MIMO suitability [20]. Moreover, its temporal spacing is shortened bya factor of 1.5.

4.1 Mathematical Representation

For easy understanding, consider the vector of one symbol. Let Xk be the input vector of size [Mx1] with be the transmitted symbols at position k and Gk= [$g_{l,\,k}$, $g_{2,\,k}$…. …. $g_{M,\,k}$] of size [NxM] be the basic matrix of FBMC where the size of the subcarrier is M and the number of FFTis N. Combining the input symbol vectors yields the signal at the transmitter [21]. The transmitted signal can be represented as the aggregate of the enter input vector with a fundamental prototype filter that's frequency shift of one any other

$$S_{Nx1}=GX \quad (3)$$

Where the overall basic matrix can be represented as **G**= [G_1, G_2, G_3.........G_k] € $\mathbb{C}^{NxMK}$ and transmit symbol at time position k with a combination of Pruned DFT spread matrix be represented as X= [X_1, ...X_k] € $\mathbb{C}$ Mx1.The modeled system is transmitted over the doubly selective channel (i.e., time and frequency selective) having time-variant impulse response along with additive white Gaussian noise vector n~CN(0,P_nI_N) where P_n denotes the noise power is represented as

$$r=HS+ n \quad (4)$$

Let $\tilde{x}_k$ of size [M/2x1] be the mapped information symbols on M/2 subcarriers, C_f be the pruned DFT spread vector [Mx M/2]. Thus, the system becomes

$$X_{k}= C_f\,\tilde{x}_k \quad (5)$$

The whole transmission after demodulation is represented as

$$y = G^HHGx + G^Hn$$
$$\approx diag\{h\}G^H G\, x + G^Hn \quad (6)$$

The estimate of the transmitted symbol with the obtained vector can be decided by means of equalizing the fading consequences of the doubly selective [22]
channel through a minimal mean square error in single delay vector channel model. This allows us to factor out the channel according to equation (4) where h € $\mathbb{C}^{LKx1}$ describes the one-tap channel, that is, the diagonal elements of G^HH G, the diagonal element represents the real value and the off-diagonal element represents the imaginary elements.

4.2 PRUNED DFT SPREAD MATRIX

The pruned DFT unfold means that the column impact of the full spreading matrix is decreased to half such that the largest top price is decreased by way of utilizing that column effect the usage of the row echelon matrix by means of mapping the QAM symbols respectively. We are also reducing the frequency-time spacing thus overhead in the reduction of column effect is adjusted. firstly, a matrix same to the quantity of subcarriers is created [23]. Then the auxiliary vector v € $\mathbb{R}^{Mx1}$ is chosen such that the i^{th} element of [v_i] corresponds to the i^{th} column of the WF matrix. To equalize the biggest element of W and make the transmit power constant implying that diagonal element $C_f^HG_k{}^HC_fG_k$ becomes one, a scaling factor u is hired as frequency spreading matrix C_f is a combination of pruned DFT and scaling value u is given by

$$C_f= \tilde{WF}_{M\times M/2}\, diag\,\{\tilde{u}\} \quad (7)$$

Where $\tilde{WF}_{MxM/2}$ € $\mathbb{C}^{MxM/2}$ represents the pruned DFT spread matrix in combination with scaling factor u€$\mathbb{R}_{MXM/2}$ and $\tilde{WF}_{MxM/2}$ is derived from largest value of full spreading matrix can therefore be expressed as

$$[\tilde{u}]_i = \frac{1}{[\sqrt{v}]i}, \text{ for } i = 1 \ldots \frac{M}{2} \quad (8)$$

The above scaling factor ensures that the inclining element is consistent (i.e.) variations in the amplitude of peak power is reduced irrespective of multicarrier effect.

4.3 DOUBLY SELECTIVE CHANNEL TDL-300ns

Larger the bandwidth smaller the sampling period than the delay spread of the channel is the notable cases in multipath scenarios, leading to frequency-selective channels [24]. While the users are in non-stop movement, the channel will become time variation channel and it's far referred because the time selectivity of the channel. in order to simulate the effects of multipath fading, a version may be created that consist of put off line with numerous tap [29]. The signal from each tap can be summed and the composite sign then represents what a real radio wave may appear like as obtained by way of receiver whilst difficulty to multipath. The impulse response of a multipath channel is by a discrete number of impulses as follows:

$$h(t, r) = \sum_{i=1}^{N} c_i(t)\delta(r - r_i) \quad (9)$$

Note that the impulse response h and coefficient c_i(t)varies with time t. There are N number of paths. There are N number of paths. consequently, to equalize the N path model with N delay line are modeled [25].

4.4 MINIMUM MEAN SQUARE ESTIMATION

To be able to do away with distortion because of signal propagation in a transmission channel, a multicarrier modulation scheme uses a channel estimation operation [30]. certainly, an estimate of the frequency reaction of the transmission channel is frequently essential to obtain frequency equalization at the output of the FFT (Fast Fourier Transform) [26]. Consequently, a scaled one-tap minimum suggests Squared error (MMSE) equalizer is used for given subcarrier position m and time position k by,

$$e_{(l,k)} = \frac{d^{*}_{m,k}}{|d|^2 + p_n} \frac{1}{1 + \sum_{i=1}^{L} \frac{1}{1 + \frac{p_n}{|d_{m,k}|^2}}} \quad (10)$$

Where h is the channel response, Pn is the noise variance The primary above is a traditional one-tap MMSE equalizer, even as the second term is a scaling aspect that guarantees that the symbol are the expected fact is about impartial, that is $E\,[\frac{y_{m,k}}{\tilde{x}_{m,k}}] = \tilde{x}_{m,k}$, Thus the estimated error equalize the multipath effect of TDL-A channel.

4.5 HERMITE FILTER

In OFDM, receiver doesn't recognize the precise time to pattern the signal due to lack of localization the various time and frequency spacing. That is a first-rate drawback that may be prolonged to create hassle of interchannel interference (ICI) and intersymbol interference (ISI). To enhance the transmission quality in multicarrier modulation (MCM) the suppression of ICI must be performed [27]. consequently, it is especially applicable to the installation a prototype filter with low time and frequency spreading, which are defined by Heisenberg uncertainty principle, as

$$\Delta T^2 = \int_{-\infty}^{\infty} t^2 |f(t)^2|\, dt, \quad (11)$$

$$\Delta F^2 = \int_{-\infty}^{\infty} f^2 |F(f)^2|\, df \quad (12)$$

$$\Delta T^2 \Delta F \geq \frac{1}{4\pi} \quad 0 \leq \Delta \leq 1 \quad (13)$$

Where ΔT *and* ΔF are the variance of the signal f in the time and frequency domain respectively [28]. The system energy in due to spreading should be minimum to avoid leakages and ISI. Subsequently true localization must be remembered of situation in multicarrier structures. Notice that well located pulses can achieve close to unit Δ, while disreputably [31] located pulses may achieve near null values of Δ.

Hermite prototype filter is expressed as

$$pHe(t) = \begin{cases} \frac{1}{\sqrt{T_0}} e^{2\pi (\frac{t}{T_0})^2} \sum_{i=(0,4,8,12,16,20)} \alpha_i D(2\sqrt{\pi}\frac{t}{T_0}) & if (-\frac{1.5}{2F}) \leq t \leq (\frac{1.5}{2F}) \\ 0 & otherwise \end{cases}$$

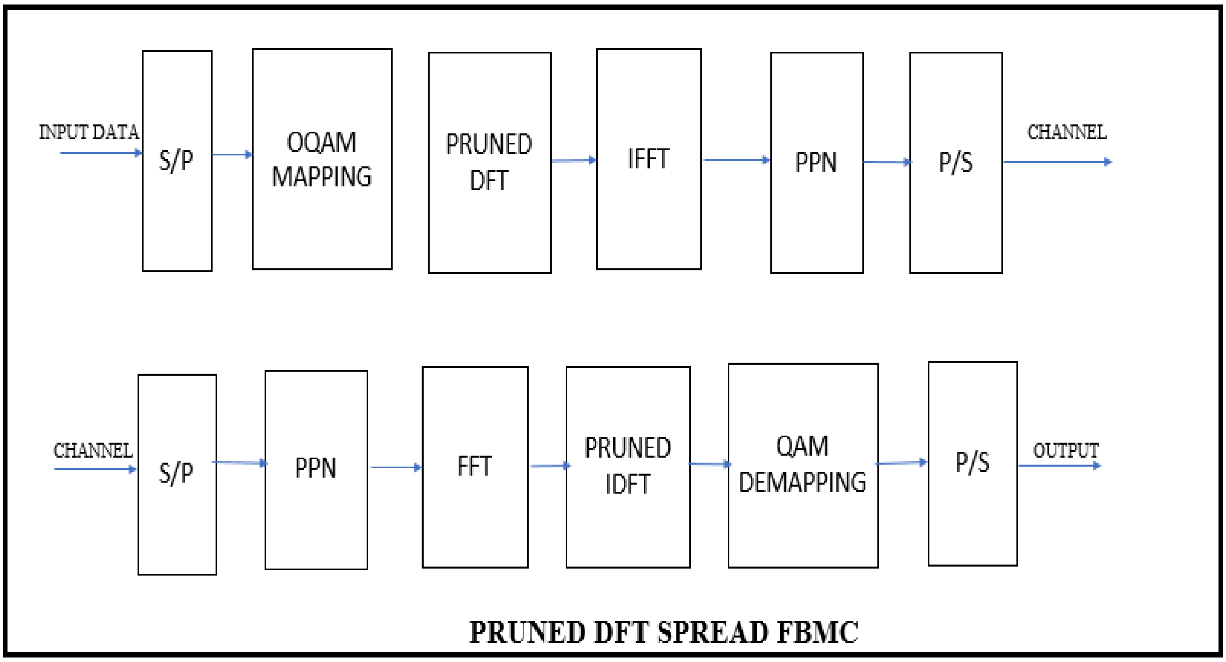

Fig. 2 Block diagram of Pruned DFT spread FBMC compared with conventional FBMC

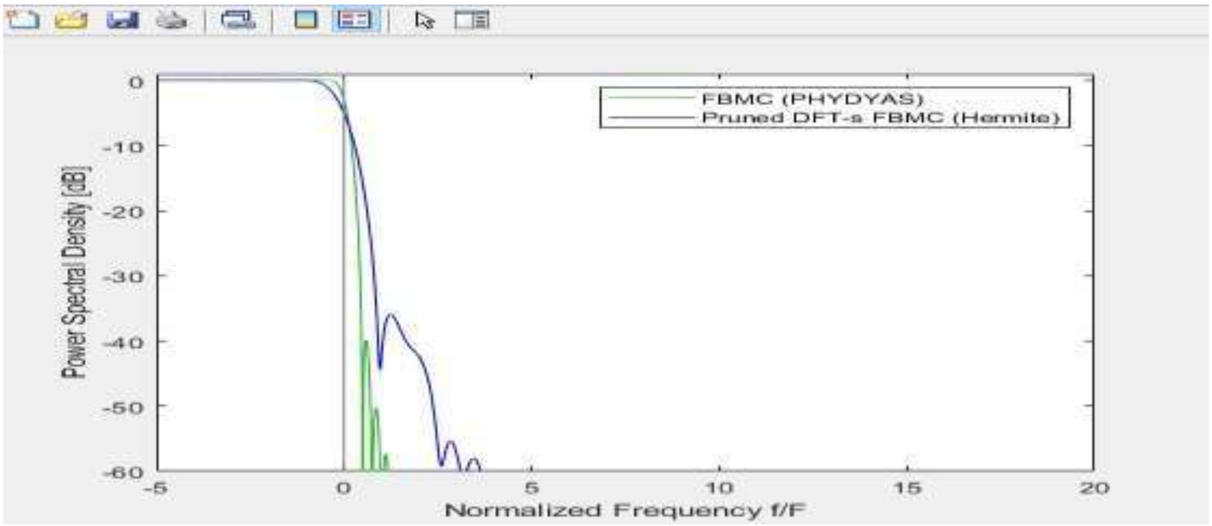

Fig. 3 PSD of pruned DFT and Conventional FBMC

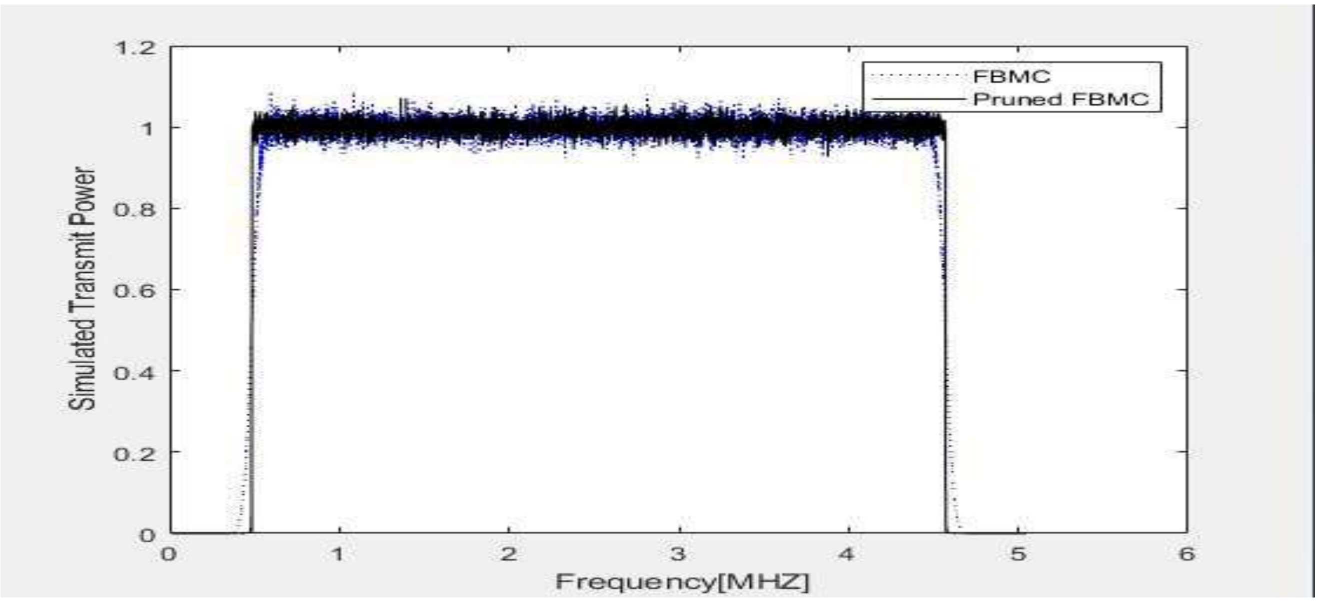

Fig. 4 Transmit power of Pruned DFT spread FBMC and conventional FBMC

5. RESULT AND DISCUSSIONS

5.1 Power spectrum

Figure 3 shows the PSD contraction of FBMC with PHYDAS filter and Pruned DFT spread FBMC with Hermite filter. In pruned DFT Spread FBMC spectral imprisonment are better than FMBC. But even with the overlapping factor of 1.56 OOB emission is poor. Since our view is based on pruning the effect of peak power and increasing the efficiency of the power amplifier, the Hermite filter outperforms others like PHYDAS and Raised cosine with a tradeoff.

Table 1 shows the Simulation factors.

Table. 1 Simulation Factors

Parameters	Value
Carrier frequency	2.5GHZ
Subcarriers size	1024
Modulation	16 QAM
FFT length	1024
Filter	PHYDAS, Hermite
Prototype factor	4,1.56
Spacing in frequency	15 KHZ
Channel used	TDL A

5.2 Transmit power

Figure 4 represents the transmit power against frequency in MHZ with N=256 and frequency spacing of 15.625 kHz, the total bandwidth is 4.5 MHZ. From the simulated result we infer that the major lobe of our proposed system is within the estimated bandwidth with a smaller number of side lobes. Thus, the proposed systems retain all the properties of conventional FBMC.

5.3 Ratio of Peak to Average Power

For a 16-QAM signal constellation with L = 256 subcarriers, the PAPR tail Distribution Function (other wards CCDF) is shown in Figure 5. As we can see, the PAPR of the standard FBMC is approximately 12 dB for a given CCDF of $1x10-1$, whereas the improvement for the pruned DFT spread is approximately 4 dB It is also fascinating to learn that the elegant DFT-spread FBMC techniques are dominated by the pruned DFT-spread FBMC in terms of PAPR performance, even when using linearly precoded OFDMA techniques to generate traditional DFT-S OFDM signals. Even while doing so results in decreased spectral efficiency, using a frequency CP further reduces the PAPR.

5.4 Bit error rate

The bit error rate implementation of the proposed and traditional systems is shown in Figure 6. The nonlinearity in transmit signal power affects the SNR, which disrupts the rate of error and raises the cost. As a result, the recommended system has the same error rate as a conventional system, as shown by the simulation result produced for SNR in the range of 0 to 15 dB. As a result, the proposed approach performs exceeds the error rate as well.

Table. 2 Results and Findings

Methods	Procedure	Findings
Proposed method	Half the inputmapping+ matrix with precoding +scaling factor +conventional FBMC	4.5 dB lesserthan FBMC
Conventionalmethod	Mapping+IFFT +Filterbank+Overlap+Sum	12 dB

Results and Findings are given in Table 2. Table 3 compares the proposed technique with other existing methods in terms of complexity, bit rate and peak to peak ratio in dB.

Table. 3 Comparison with Existing Techniques

Techniques	PAPR Obtained	Complexity	BER
Pruned DFT based reduction technique	Reduced to 7.5 dB	Involves only pruned DFT and Hermite filter so less computationalcomplexity	Same as FBMC
DFT-based Scheme with block repetition[1]	8.5 dB	It is based on block repetition leads tohigher computation	Equal as FBMC
Alamouti code based DFT spreading [5]	8 dB	Requires frequency reversal Alamouti code with phase condition but the problem occurs in decoding.	Lesser BER thanother techniques
GDFT with single carrier phase conditioneffect [4]	8 dB	Uses different phase conditions with in-phase and quadrature terms. Phasecriterion requires careful designing methods.	Not mentioned

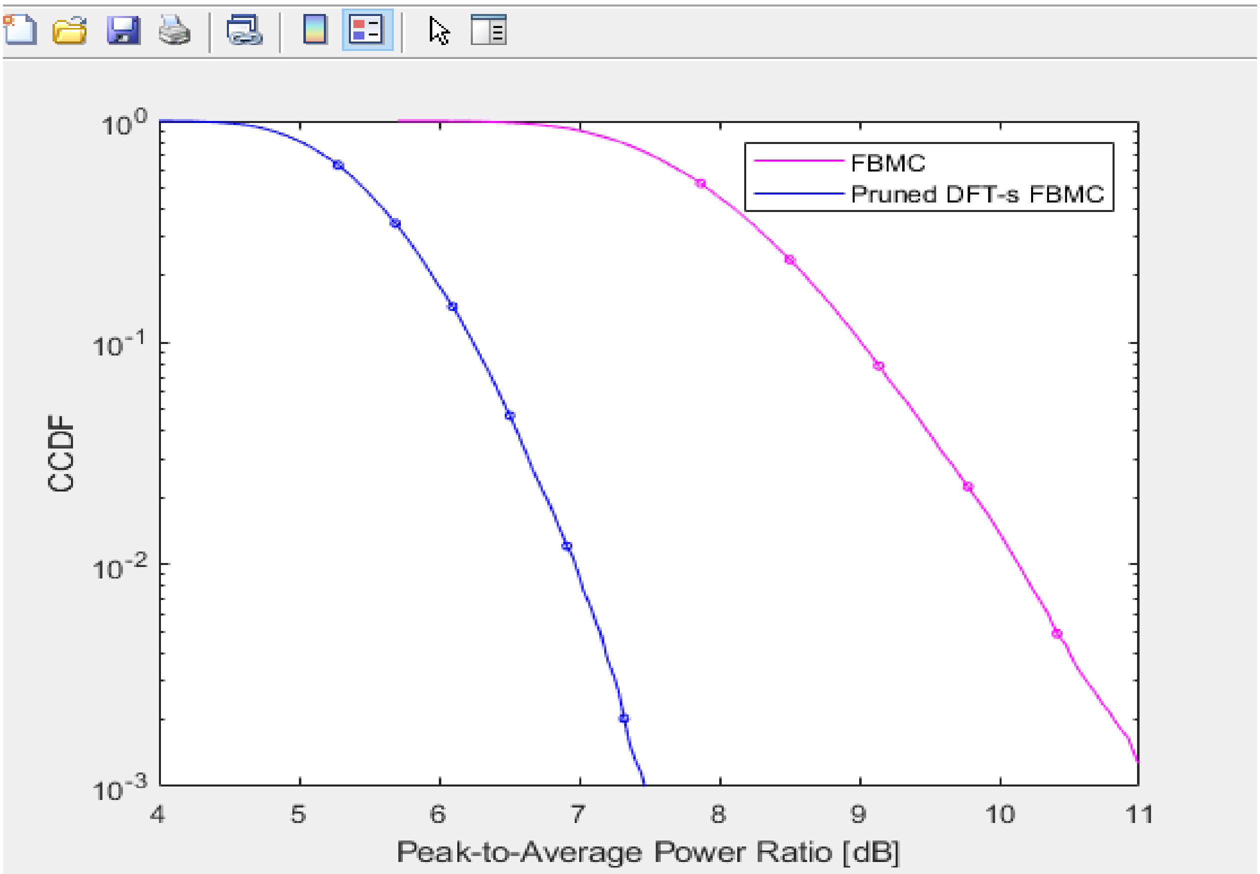

Fig. 5 PAPR of FBMC and pruned DFT spread FBMC

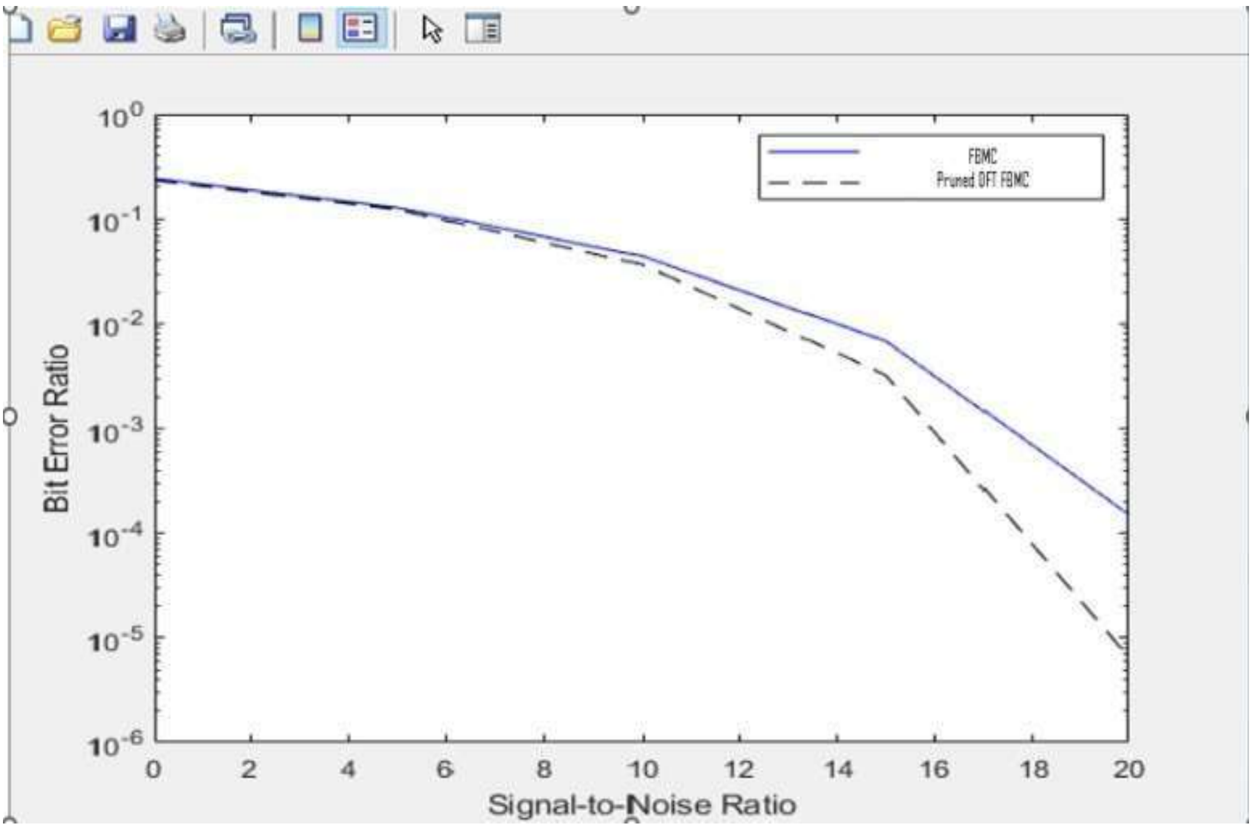

Fig. 6 BER of Pruned DFT spread FBMC and conventional FBMC

6 CONCLUSION

According to all these simulated results and theoretical research, the proposed pruned DFT spread FBMC uses a precoding matrix that takes advantage of the spreading matrix's column impact to cancel out the effects of QAM and IFFT. Scaling is also used to make it more constrained. As a result, the peak power to average power ratio decreases causing the power amplifier to operate linearly. The system is then further examined in one of the TDL-A channel models temporal and frequency selective channels. Equalization is performed using a one-tap MMSE. It is hence resistant to the Doppler effect and the fading effect. Finally, the Hermite filteris used in addition to PHYDAS in order to achieve good time and frequency localization. A good BER rate is also the result of reduced transmits power. The typical method still has the same latency and complexity. As a result, the suggested Pruned DFTspread FBMC offers a fast data rate, good frequency localization, fewer spectral leakages, and a nearly 4 dB reduction in PAPR. Thus, 5G networks can adopt this contested waveform modulation technique.

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AUTHORS

R. Sittalatchoumy has 25 years of experience in the field of academic and research activities. She obtained her BTech, (Electronics and Communication Engineering) degree from Pondicherry University, Puducherry, ME, (Communication Systems) and PhD, degree from Anna University, Chennai. Her area of interest is Wireless Sensor Networks, IOT based system design, and Communication Networks. She is a Life Member of ISTE.

Corresponding Author Email: sittalatchoumy@gmail.com

Malarvizhi Muthuramalingam has received her Bachelor of Engineering in department of Electronics and Communication, in 2020 from University College of Engineering–BIT campus, Trichy. She completed her master's in communication systems from the College of Engineering – Guindy, Chennai in 2022. She is currently working as a Project officer at Shiv Nadar University, Chennai, and doing research on speech processing. Her area of interest are signal processing and Wireless communication.

Email: malarvizhibh9903@gmail.com